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Vehicle-Vehicle Energy Interaction Converter of Electric Vehicles: A Disturbance Observer Based Sliding Mode Control Algorithm

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Abstract—The electric vehicle technology is one of the most promising candidates to reduce fuel consumption and CO₂ emission. Although electric vehicles have been widely promoted by governments around the world, their development is seriously hampered due to charger unavailability and range anxiety. Based on this, this paper designs an energy interaction converter between two electric vehicles, which is controlled through disturbance observer based sliding mode control algorithm. For this converter, three main demands should be satisfied, i.e., high power density, weak source and constant power load. Therein, weak source whose minimum short circuit ratio (SCR) belongs to [2,3], is always called weak grid. Firstly, the equivalent impedance switching process is introduced to eliminate the impact of weak source. Meanwhile, the equivalent six channel interleaved floating dual boost converter is chosen to satisfy the high power density demand, whose generalized state-space function is further built to provide an indispensable preprocessing for following controller design. Moreover, in order to solve the problem regarding low frequency/sub-synchronous oscillation caused through constant power load feature regarding the energy consumption vehicle and weak source feature regarding the energy supply vehicle, a disturbance observer based sliding mode control algorithm is proposed through using generalized state-space function to provide standard DC power with both constant voltage and power. Furthermore, the proportional-resonant controller is proposed to solve the current sharing problem among six parallel channels, which reduces the heat loss and improves the service life of the device. Finally, simulation and experimental results verify the high performance of the proposed control algorithm.

Index Terms—electric vehicle, energy interaction converter, impedance switching, sliding mode control.

I. INTRODUCTION

THE Paris Conference in 2015 has provided one guide to restrict climate variation “well below 2 degrees C” [1], which has triggered the studies for clean alternative fuels for transportation. To this end, the electric vehicle technology has

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become one of the most promising candidates at present [2]-[3]. Although the electric vehicle has been widely promoted by governments around the world, three main problems still hinder the development of electric vehicles, i.e., charger unavailability, range anxiety and high prices. Therein, the high price has been alleviated through subsidized charging programmes and tax breaks [4]-[5]. However, it is urgent for scholars to deal with charger unavailability and range anxiety. Based on this, this paper designs an energy interaction converter between two electric vehicles, which is controlled through disturbance observer based sliding mode control algorithm.

Once battery mileage problem such as lack of electricity in the middle of the way occurs in electric vehicles, vehicle owners could only rescue and wait for rescue through mobile communication devices, which reduces the buying enthusiasm regarding electric vehicles. In order to solve this problem, it is advisable that electric vehicles charge each other through portable energy interaction converter. Therein, the energy supply vehicle can be regarded as one weak source, and the energy consumption vehicle always adopts constant power charge mode, which can be regarded as one constant power load [6]. However, the instability caused through weak source and constant power load has been widely reported such as low-frequency oscillation and sub-synchronous oscillation [7]-[8]. To sum up, three major challenges such as high power density, weak source and constant power load should be solved.

For constant power loads, plenty of scholars proposed numerous approaches, which could be divided into linear control strategy and nonlinear control strategy [7], [9]-[20]. From the viewpoint of the linear control strategy, the passive damping control technology was proposed to achieve the system stability operation through adding passive components such as capacitors/resistors [9]-[10]. However, the additional physical components were bound to increase the cost and consumption of the system. Based on this, the active damping technology was proposed through virtual impedance injection, which could improve the stability margin and response speed of the system at the same time [11]-[12]. However, the foresaid linear control technologies are based on the linear model under small signal, which is difficult for scholars to adopt in the vehicle-vehicle energy interaction converter of electric vehicles [13].

Different from the linear control strategy, the nonlinear control technology could realize fast energy interaction control among main grid and loads [7]. Firstly, feedback linearization

technique was proposed to eliminate the negative impedance characteristic and nonlinear term caused through constant power loads [14]-[15]. However, compared with other nonlinear control strategies, this technique had obvious defects such as slow dynamic response and unclear disturbance mechanism. To that end, the conventional input-output linearization strategy was proposed to realize the safe and stable operation of constant power loads, whose essence was to transform non-minimum phase system into minimum phase system [16]. Nevertheless, it was difficult to determine the accurate equivalent impedance of the electric system. The real-time nonlinear model predictive controller was proposed for direct yaw moment control of distributed drive electric vehicles, which achieved real-time optimization [17]-[18]. However, this method focused more on Magic Formula (MF) tire model. Furthermore, the model predictive control based on high-order sliding mode observer was proposed to realize the stable operation of boost converter with constant power loads. High order sliding mode observer could eliminate the impact of negative impedance and circuit parameter uncertainty, which was, however, required very high computing power [19]. Clearly, the processor in the convenient energy interaction converter was difficult to satisfy the relevant requirements. For the conventional boost converter with unknown line parameters and constant power loads, the disturbance observer based on back-stepping was proposed to achieve accurate tracking and stable operation under disturbance in the literature [20]. Nevertheless, it needed to make strict assumptions about the unknown types of line parameters, which restricted its application in practical systems. Recently, the sliding mode control approach was proposed to ensure the stable operation of step-up transformer under constant power loads, which was regarded as an active stabilization control [21]-[22]. Firstly, the fixed frequency sliding mode control strategy with constant power load was proposed to ensure the stable operation of the system [21]. However, it required additional current sensors such that the hardware cost and equivalent output impedance were increased. Furthermore, the robust sliding mode control strategy was proposed for the conventional boost converter in the literature [22]. Therein, it was very sensitive to the DC source voltage and was necessary to assume that the supply side voltage of the system was constant, which was difficult for practical electric vehicles. Thus, it is urgent for scholars to propose a suitable control strategy for the energy interaction converter of electric vehicles.

In order to achieve the energy interaction between two electric vehicles, this paper designs an energy interaction converter controlled through disturbance observer based sliding mode control algorithm. The main advantages of the proposed method are shown as follows:

- 1) The energy interaction converter with weak source and constant power load is switched to the parallel six channel interleaved floating dual boost converter with partial unknown circuit parameters, which is further built as one state-space function with unknown parameters. With these effects, the demands regarding high power density and weak source can be satisfied;
- 2) Based on the foresaid state-space function, an energy

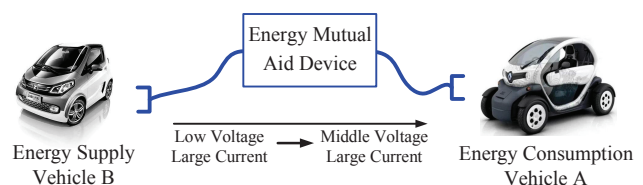


Fig. 1: Portable electric vehicle energy interaction converter.

interaction converter controlled through disturbance observer based sliding mode control algorithm is designed in this paper. Under this approach, the demand regarding constant power load can be satisfied. Furthermore, the proportional-resonant controller is proposed to solve the current sharing problem caused through proposed six parallel channels, which reduces the heat loss and improves the service life of the energy interaction converter.

The rest of the paper is shown as follows. In Section II, the state-space function with partial unknown parameters regarding energy interaction converter consisting of weak source and constant power load is built. Furthermore, an energy interaction converter controlled through disturbance observer based sliding mode control algorithm is designed in Section III. Moreover, the proportional-resonant controller is proposed to achieve accurate current sharing in Section IV. Meanwhile, the simulation and experiment results are provided to validate the performance of the proposed approach in Section V and Section VI. Eventually, this paper is concluded in Section VII.

II. MODIFIED SIX CHANNEL INTERLEAVED FLOATING DUAL BOOST CONVERTER AND ITS STATE-SPACE FUNCTION

If the battery energy of the electric vehicle is insufficient and cannot be charged nearby through the charging station, the electric vehicle owner can use the portable electric vehicle energy interaction converter shown in Fig. 1, to obtain power energy from the electric vehicle whose battery is plentiful. Among them, the electric vehicle with insufficient electric energy can be defined as the energy consumption vehicle A, and the electric vehicle with abundant electric energy is defined as the energy supply vehicle B. Since each electric vehicle has four to six batteries and the output voltage of each battery is 15V, the practical output voltage regarding the energy supply vehicle B is approximately 60V. Meanwhile, the input voltage regarding the energy consumption vehicle A is 250V [6]. In order to satisfy the fast charge between two electric vehicles, the transmission power is expected to be more than 20kW. Thus, the high power density should be achieved.

Since the supply power source regarding electric vehicles belongs to the weak source, the practical source for the energy interaction converter can be equivalent to the Thevenin equivalent circuit, which is shown in Fig. 2 [23]. Therein, equivalent inductance can be represented as $L_g = 1/SCR[p.u.]$ [24], SCR represents the minimum short circuit ratio, which is often used to characterize the strength of the grid. According to IEEE 1204-1997 standard, the system belongs to weak grid if $SCR \in [2, 3]$ [25].

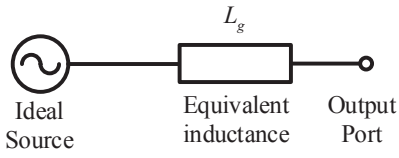


Fig. 2: Thevenin equivalent of weak source.

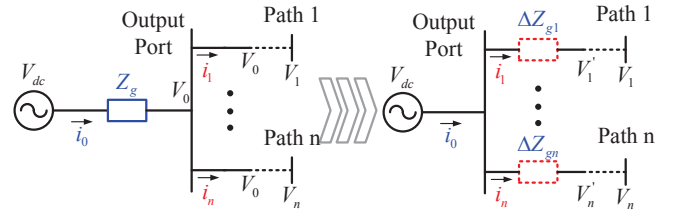


Fig. 4: Equivalent impedance switching process

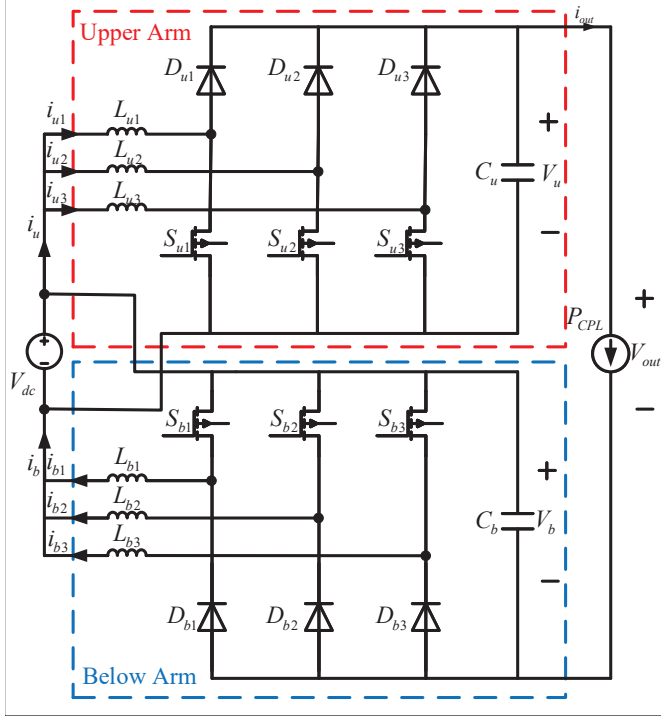


Fig. 3: Hardware topology of the energy interaction converter

Due to the high power density demand, the energy interaction converter adopts the six channel interleaved floating dual boost converter in this paper, which is shown in Fig. 3, where the DC source V_{dc} is the weak source of the energy supply vehicle B and the energy consumption vehicle A is regarded as one constant power load P_{CPL} . L_{u1} to L_{u3} represent inductances of the three channels in the upper bridge arm, respectively. L_{b1} to L_{b3} represent inductances of the three channels in the below bridge arm, respectively. Noting that L_{u1} to L_{u3} and L_{b1} to L_{b3} belong to the inner structure regarding the converter. i_{u1} to i_{u3} represent currents of the three channels in the upper bridge arm, respectively. i_{b1} to i_{b3} represent currents of the three channels in the below bridge arm, respectively. V_u , i_u and C_u represent the output voltage, current and capacitor of the upper bridge arm regarding the energy interaction converter, respectively. V_b , i_b and C_b represent the output voltage, current and capacitor of the below bridge arm regarding the energy interaction converter, respectively. Noting that $i_{out} = P_{CPL}/V_{out}$.

In order to eliminate the impact of the equivalent inductance of the weak source (L_g) and facilitate the controller design, the equivalent impedance switching process can be proposed in this section, which is shown in Fig. 4. Due to the existence of current sharing controller, the current flowing through each path is the same, i.e., $i_1 = i_2 = \dots = i_n$. According

to our previous literature [26], the equivalent inductance is transformed into the same inductance in each path, e.g., $\Delta L_{g1} = \dots = \Delta L_{gn}$. Since the model of each battery regarding electric vehicle is unknown, it is difficult to acquire the equivalent inductance in advance, that is, $\Delta L_{g1} = \dots = \Delta L_{gn}$ is unknown. Thus, the weak source demand should be achieved through embedding equivalent inductance to state-space function of the energy interaction converter.

To sum up, according to Kirchhoff voltage/current law and model average modeling technology, the average model of the upper bridge arm is shown as follows :

$$(L_{ui} + \Delta L_{gui}) \frac{di_{ui}}{dt} = V_{dc} - (1 - u_{ui}) V_u \quad (1)$$

$$C_u \frac{dV_u}{dt} = \sum_{i=1}^3 i_u (1 - u_{ui}) - i_{out} \quad (2)$$

where u_{ui} represents the duty cycle of the i^{th} channel of the upper arm of the energy interaction converter, and ΔL_{gui} represents the unknown equivalent power inductance of the i -channel of the upper arm. Since the energy interaction converter is symmetrical, $L_{u1} = L_{u2} = L_{u3}$. At the same time, due to the existence of averaging controller, $i_{u1} = i_{u2} = i_{u3}$. Therefore, the generalized reduced order average model of the upper arm is as follows:

$$(L_u + \Delta L_{gu}) \frac{di_u}{dt} = V_{dc} - (1 - u_u) V_u \quad (3)$$

$$(C_u + \Delta C_u) \frac{dV_u}{dt} = i_u (1 - u_u) - i_{out} \quad (4)$$

where $L_u = \frac{1}{3} L_{ui}$ represents the primary inductance of the upper arm equivalent boost converter; $\Delta L_{gu} = \frac{1}{3} \Delta L_{gui}$ represents equivalent weak source inductance of upper bridge arm; ΔC_u represents capacitance uncertainty caused by parasitic capacitance of upper bridge arm; u_u represents equivalent duty cycle of upper arm. i.e., $u_u = u_{ui}$. Noting that the state space model in this paper is still one state-space function with partial unknown parameters. In order to solve these unknown parameters, one disturbance observer is designed in Section III. Similarly, the generalized reduced order average model of the lower arm is shown as follows:

$$(L_b + \Delta L_{gb}) \frac{di_b}{dt} = V_{dc} - (1 - u_b) V_b \quad (5)$$

$$(C_b + \Delta C_b) \frac{dV_b}{dt} = i_b (1 - u_b) - i_{out} \quad (6)$$

where $L_b = \frac{1}{3}L_{bi}$ represents the primary inductance of the lower arm equivalent boost converter; $\Delta L_{gb} = \frac{1}{3}\Delta L_{gbi}$ represents equivalent weak source inductance of lower bridge arm; ΔC_b represents capacitance uncertainty caused by parasitic capacitance of lower bridge arm; u_b represents equivalent duty cycle of lower arm. i.e., $u_b = u_{bi}$. There is no doubt that $L_u = L_b = L$. According to Kirchhoff voltage law, it can be seen that:

$$V_{out} = V_u + V_b - V_{dc} \quad (7)$$

Therefore, the control objective of this paper is to accurately control the output voltage of the upper/lower bridge arms, i.e. V_u and V_b , to ensure that the output voltage of the energy interaction converter can reach the rated input voltage of distributed generator. To this end, the output voltage of the upper/lower arm should be controlled to $V_u = V_b = V_{ref}^*$ where $V_{ref}^* = (V_{ref} + V_{dc})/2$. Therein, V_{ref} represents the whole output voltage of the portable electric vehicle energy interaction converter, V_{ref}^* represents the output voltage of the upper arm or below arm regarding the portable electric vehicle energy interaction converter. For this energy interaction converter, the input variables are current (i_u and i_b) and voltage (V_u , V_b and V_{dc}). Meanwhile, the output variables are switching signals (u_{ph1} to u_{ph6}). In order to satisfy the demands regarding weak source and constant power load, three controllers should be designed. Therein, the disturbance observer should be designed to solve the partial unknown parameters, and sliding mode controller should be designed to make the output voltage of the upper/lower arm be controlled to $V_u = V_b = V_{ref}^*$. Finally, the proportional-resonant controller is proposed to solve the current sharing problem caused through proposed six parallel channels.

III. DISTURBANCE OBSERVER BASED SLIDING MODE CONTROL ALGORITHM

In order to satisfy the constant power load demand, the disturbance observer based sliding mode control algorithm is proposed in this section, which should provide stable output voltage of the modified six channel interleaved floating dual boost converter under variation of source and load. In order to considering the constant power load in terms of linear approach, the generalized average model (3)-(6) proposed in the foresaid section should be transformed into one linear standard system to design sliding mode control based on disturbance observer. Firstly, a series of state variables are defined to describe the energy interaction converter

$$x_1 = 0.5Li_u^2 + 0.5C_uV_u^2 \quad (8)$$

$$x_2 = V_{dc}i_u \quad (9)$$

$$x_3 = 0.5Li_b^2 + 0.5C_bV_b^2 \quad (10)$$

$$x_4 = V_{dc}i_b \quad (11)$$

where x_1 and x_3 represent the energy of the upper/lower arm of the energy interaction converter, and x_2 and x_4 represent the output power of the upper/lower arm of the energy interaction converter. Then, the derivative calculation is carried out and

the following results are obtained

$$\dot{x}_1 = Li_u\dot{i}_u + C_uV_u\dot{V}_u \quad (12)$$

$$\dot{x}_2 = V_{dc}\dot{i}_u \quad (13)$$

$$\dot{x}_3 = Li_b\dot{i}_b + C_bV_b\dot{V}_b \quad (14)$$

$$\dot{x}_4 = V_{dc}\dot{i}_b \quad (15)$$

By substituting equation (3)-(6) into equation (12)-(15):

$$d_1 = -V_u i_{out} - \frac{\Delta L_{gu}}{L + \Delta L_{gu}} [V_{dc} - (1 - u_u) V_u] - \frac{\Delta C_u V_u}{C_u + \Delta C_u} [(1 - u_u) i_u - i_{out}] \quad (16)$$

$$d_2 = \frac{-V_{dc}\Delta L_{gu}}{L(L + \Delta L_{gu})} [V_{dc} - (1 - u_u) V_u] \quad (17)$$

$$d_3 = -V_b i_{out} - \frac{\Delta L_{gb}}{L_b + \Delta L_{gb}} [V_{dc} - (1 - u_b) V_b] - \frac{\Delta C_b V_b}{C_b + \Delta C_b} [(1 - u_b) i_b - i_{out}] \quad (18)$$

$$d_4 = \frac{-V_{dc}\Delta L_{gb}}{L(L + \Delta L_{gb})} [V_{dc} - (1 - u_b) V_b] \quad (19)$$

$$h_1 = \frac{V_{dc}^2}{L} - \frac{(1 - u_u) V_{dc} V_u}{L} \quad (20)$$

$$h_2 = \frac{V_{dc}^2}{L} - \frac{(1 - u_b) V_{dc} V_b}{L} \quad (21)$$

Therefore, the equation of state (12)-(15) can be rewritten:

$$\dot{x}_1 = x_2 + d_1 \quad (22)$$

$$\dot{x}_2 = h_1 + d_2 \quad (23)$$

$$\dot{x}_3 = x_4 + d_3 \quad (24)$$

$$\dot{x}_4 = h_2 + d_4 \quad (25)$$

where h_1 and h_2 represent the virtual control quantities of the upper and lower arms respectively. It should be noted that equations (22)-(25) are differential homeomorphic maps of the primitive system (3)-(6) [27]. Based on the operation mechanism of the energy interaction converter, the following components can be ignored, i.e., $[V_{dc} - (1 - u_u) V_u]$, $[(1 - u_u) i_u - i_{out}]$, $[V_{dc} - (1 - u_b) V_b]$ and $[(1 - u_b) i_b - i_{out}]$. Therefore, disturbances d_1 and d_2 can be simplified as follows:

$$d_1 = -V_u i_{out} \quad (26)$$

$$d_3 = -V_b i_{out} \quad (27)$$

Using equations (16)-(21), the actual control variables of the controller can be obtained as follows:

$$u_u = 1 - \frac{V_{dc}^2 - Lh_1}{V_{dc}V_u} \quad (28)$$

$$u_b = 1 - \frac{V_{dc}^2 - Lh_2}{V_{dc}V_b} \quad (29)$$

After the coordinate transformation of the differential homeomorphism mapping, the objectives of the controller are transformed from V_{out} tracking V_{ref} to state variables x_1 and x_3 , which converge gradually to their rated values, i.e. x_{1ref}

and x_{3ref} , which is shown as follows:

$$x_{1ref} = 0.5L i_{uref}^2 + 0.5C_u V_{uref}^2 \quad (30)$$

$$x_{2ref} = V_{dc} i_{uref} \quad (31)$$

$$x_{3ref} = 0.5L i_{bref}^2 + 0.5C_b V_{bref}^2 \quad (32)$$

$$x_{4ref} = V_{dc} i_{bref} \quad (33)$$

where $V_{uref} = V_{bref} = V_{ref}^*$, i_{uref} and i_{bref} represent the input current reference value of the upper/lower bridge arm, respectively. Taking into account the conservation of input/output power, i_{uref} and i_{bref} can be expressed:

$$i_{uref} = i_{bref} = \frac{V_{ref}^* i_{out}}{V_{dc}} \quad (34)$$

Since the disturbances d_1 to d_4 are composed of uncertainties caused by output current and weak source/parasitic capacitance, they and their derivatives have extremum, i.e., $d_{i\max} = \sup_{t>0} |d_i(t)|$ and $\dot{d}_{i\max} = \sup_{t>0} |\dot{d}_i(t)|$. At the same time, the final value of its derivative tends to zero in steady state. Based on equations (26) - (27), the instantaneous value of the output current of the energy interaction converter can be obtained by disturbances d_1 and d_3 . Therefore, rating x_{1ref} to x_{4ref} of the state variable can be accurately obtained through observing d_1 and d_3 . Based on this, a disturbance observer is designed in this paper

$$\begin{cases} \hat{d}_1 = H_{d1}x_1 + \alpha_1 \\ \dot{\alpha}_1 = -H_{d1}(x_2 + \hat{d}_1) \end{cases} \quad (35)$$

$$\begin{cases} \hat{d}_2 = H_{d2}x_2 + \alpha_2 \\ \dot{\alpha}_2 = -H_{d2}(h_1 + \hat{d}_2) \end{cases} \quad (36)$$

$$\begin{cases} \hat{d}_3 = H_{d3}x_3 + \alpha_3 \\ \dot{\alpha}_3 = -H_{d3}(x_4 + \hat{d}_3) \end{cases} \quad (37)$$

$$\begin{cases} \hat{d}_4 = H_{d4}x_4 + \alpha_4 \\ \dot{\alpha}_4 = -H_{d4}(h_2 + \hat{d}_4) \end{cases} \quad (38)$$

where \hat{d}_1 to \hat{d}_4 represent the observed values of disturbance d_1 to d_4 ; H_{d1} to H_{d4} represent the positive observation gains; α_1 to α_4 represent the internal variables of the observer. Using equations (35)-(38), the observer error dynamic characteristics are as follows:

$$\dot{e}_{d1} = -H_{d1}e_{d1} + \dot{d}_1 \quad (39)$$

$$\dot{e}_{d2} = -H_{d2}e_{d2} + \dot{d}_2 \quad (40)$$

$$\dot{e}_{d3} = -H_{d3}e_{d3} + \dot{d}_3 \quad (41)$$

$$\dot{e}_{d4} = -H_{d4}e_{d4} + \dot{d}_4 \quad (42)$$

where $e_{di} = d_i - \hat{d}_i$ represents observer error. The following energy functions are constructed

$$Q(e_{d1}, e_{d2}, e_{d3}, e_{d4}) = 0.5 \sum_{i=1}^4 e_{di}^2 \quad (43)$$

Therefore, the following inequality can be obtained

$$\begin{aligned} \dot{Q}(e_{di}) &= \sum_{i=1}^4 \left(-H_{di}e_{di}^2 + e_{di}\dot{d}_i \right) \\ &\leq \sum_{i=1}^4 \left(-H_{di}|e_{di}|^2 + |e_{di}|\dot{d}_{i\max} \right) \\ &= -\sum_{i=1}^4 |e_{di}| \left(H_{di}|e_{di}| - \dot{d}_{i\max} \right) \end{aligned} \quad (44)$$

Therefore, in a finite time, the estimation error is finite and the boundary is shown as follows:

$$|e_{di}| \leq \sigma_d \quad (45)$$

where $\sigma_d = \max(\dot{d}_{i\max}/H_{di})$. Since unknown parameters are embedded into the state space model, the disturbance observer based sliding mode control algorithm should be proposed in this paper. Based on equations (26)-(27) and (30)-(34), the estimated reference values of the state variables are shown as follows:

$$\hat{x}_{1ref} = 0.5L \frac{\hat{d}_1^2}{V_{dc}^2} + 0.5C_u V_{ref}^{*2} \quad (46)$$

$$\hat{x}_{2ref} = -\hat{d}_1 \quad (47)$$

$$\hat{x}_{3ref} = 0.5L \frac{\hat{d}_3^2}{V_{dc}^2} + 0.5C_b V_{ref}^{*2} \quad (48)$$

$$\hat{x}_{4ref} = -\hat{d}_3 \quad (49)$$

Furthermore, a sliding mode controller based on disturbance observer is proposed, and its sliding surface is shown as follows:

$$s_1 = a_1 e_{x1} + e_{x2} - \dot{\hat{x}}_{1ref} \quad (50)$$

$$s_2 = a_2 e_{x3} + e_{x4} - \dot{\hat{x}}_{3ref} \quad (51)$$

Among them, $e_{xi} = x_i - x_{iref}$ is called the state deviation; $\dot{\hat{x}}_{1ref}$ and $\dot{\hat{x}}_{3ref}$ represent the derivatives of \hat{x}_{1ref} and \hat{x}_{3ref} . In order to ensure that the sliding surfaces s_1 and s_2 converge to zero, the following controllers are designed:

$$\begin{aligned} h_1 &= -a_1 \left(e_{x2} - \dot{\hat{x}}_{1ref} \right) + \ddot{\hat{x}}_{1ref} - \dot{\hat{d}}_1 - \hat{d}_2 \\ &\quad - H_{s1} \text{sgn}(s_1) - H_{s2} s_1 \end{aligned} \quad (52)$$

$$\begin{aligned} h_2 &= -a_2 \left(e_{x4} - \dot{\hat{x}}_{3ref} \right) + \ddot{\hat{x}}_{3ref} - \dot{\hat{d}}_3 - \hat{d}_4 \\ &\quad - H_{s3} \text{sgn}(s_2) - H_{s4} s_2 \end{aligned} \quad (53)$$

where H_{s1} to H_{s4} represent the gains of positive definite sliding mode controller. To sum up, the convergence and stability of the controller can be obtained by the following theorem:

Theorem 1: If the following condition is satisfied: 1) $(H_{s1} - H_{s2}|s_1|) > (1 + a_1)\sigma_d$ and $(H_{s3} - H_{s4}|s_2|) > (1 + a_2)\sigma_d$; 2) a sufficiently large H_{\min} is selected, the energy interaction converter based on equations (28)-(29) is asymptotically stable, and its output voltage V_{out} can track up to V_{ref} .

Proof: Applying equations (22)-(25), (39)-(42) and (46)-(49), the derivatives of slip surfaces s_1 and s_2 are shown as follows:

$$\dot{s}_1 = a_1 e_{d1} + e_{d2} - H_{s1} \text{sgn}(s_1) - H_{s2} s_1 \quad (54)$$

$$\dot{s}_2 = a_2 e_{d3} + e_{d4} - H_{s3} \text{sgn}(s_2) - H_{s4} s_2 \quad (55)$$

Define the standard Lyapunov equation:

$$V(s_1, s_2) = 0.5s_1^2 + 0.5s_2^2 \quad (56)$$

Based on this, the derivative of $V = V(s_1, s_2)$ is shown as follows:

$$\begin{aligned} \dot{V} &= s_1 \dot{s}_1 + s_2 \dot{s}_2 \\ &= -H_{s1} |s_1| - H_{s2} s_1^2 - H_{s3} |s_3| - H_{s4} s_2^2 \\ &\quad + (a_1 e_{d1} + e_{d2}) s_1 + (a_2 e_{d3} + e_{d4}) s_2 \\ &\leq -H_{s1} |s_1| - H_{s2} s_1^2 - H_{s3} |s_3| - H_{s4} s_2^2 \\ &\quad + (1 + a_1) \sigma_d s_1 + (1 + a_2) \sigma_d s_2 \\ &= -[H_{s1} + H_{s2} |s_1| - (1 + a_1) \sigma_d] |s_1| \\ &\quad - [H_{s3} + H_{s4} |s_2| - (1 + a_2) \sigma_d] |s_2| \quad (57) \end{aligned}$$

Therefore, if $(H_{s1} - H_{s2} |s_1|) > (1 + a_1) \sigma_d$ and $(H_{s3} - H_{s4} |s_2|) > (1 + a_2) \sigma_d$, the state error of the system converges asymptotically to the defined sliding surfaces $s_1 = 0$ and $s_2 = 0$. When H_{d1} to H_{d4} is large enough, σ_d can be arbitrarily small, and H_{s1} to H_{s4} can also be selected to be relatively small to alleviate the sliding mode chattering problem. Based on equations (50)-(51), if $s_1 = 0$ and $s_2 = 0$, let

$$e_{x2} = -a_1 e_{x1} + \dot{x}_{1ref} \quad (58)$$

$$e_{x4} = -a_2 e_{x3} + \dot{x}_{3ref} \quad (59)$$

$$\dot{e}_{x1} = e_{x2} + e_{d1} - \dot{x}_{1ref} \quad (60)$$

$$\dot{e}_{x3} = e_{x4} + e_{d3} - \dot{x}_{3ref} \quad (61)$$

By substituting equations (57)-(58) into equations (59)-(60) and combining equations (39)-(42), it can be seen that the sliding mode dynamics of the energy interaction converter based on disturbance observer is shown as follows:

$$\dot{e} = \mathbf{A}e + \mathbf{B}\dot{d} \quad (62)$$

where $\dot{e} = [\dot{e}_{x1}, \dot{e}_{d1}, \dot{e}_{d2}, \dot{e}_{x3}, \dot{e}_{d3}, \dot{e}_{d4}]^T$ and $\dot{d} = [\dot{d}_1, \dot{d}_2, \dot{d}_3, \dot{d}_4]$. \mathbf{A} and \mathbf{B} are shown as follows:

$$\mathbf{A} = \begin{bmatrix} -a_1 & 1 & 0 & 0 & 0 & 0 \\ 0 & -H_{d1} & 0 & 0 & 0 & 0 \\ 0 & 0 & -H_{d2} & 0 & 0 & 0 \\ 0 & 0 & 0 & -a & 1 & 0 \\ 0 & 0 & 0 & 0 & -H_{d3} & 0 \\ 0 & 0 & 0 & 0 & 0 & -H_{d4} \end{bmatrix}$$

$$\mathbf{B} = \begin{bmatrix} 0 & 0 & 0 & 0 \\ 1 & 0 & 0 & 0 \\ 0 & 1 & 0 & 0 \\ 0 & 0 & 0 & 0 \\ 0 & 0 & 1 & 0 \\ 0 & 0 & 0 & 1 \end{bmatrix}$$

Define the following Lyapunov equation:

$$V_e = Q(e_{di}) + 0.5e_{x1}^2 + 0.5e_{x3}^2 \quad (63)$$

Its derivative is shown below

$$\begin{aligned} \dot{V}_e &= \dot{Q}(e_{di}) + e_{x1} \dot{e}_{x1} + e_{x3} \dot{e}_{x3} \\ &= \dot{Q}(e_{di}) + (-a_1 e_{x1}^2 + e_{x1} e_{d1}) + (-a_3 e_{x3}^2 + e_{x3} e_{d3}) \\ &= \sum_{i=1}^4 \left(-H_{di} e_{di}^2 + e_{di} \dot{d}_i \right) + (-a_1 e_{x1}^2 + e_{x1} e_{d1}) \\ &\quad + (-a_3 e_{x3}^2 + e_{x3} e_{d3}) \quad (64) \end{aligned}$$

Using Young inequality, the following equations can be obtained

$$\begin{aligned} \dot{V}_e &\leq -(H_{d1} - 1) e_{d1}^2 - H_{d2} e_{d2}^2 - (H_{d3} - 1) e_{d3}^2 - H_{d4} e_{d4}^2 \\ &\quad - (a_1 - 0.5) e_{x1}^2 - (a_3 - 0.5) e_{x3}^2 + 0.5 \sum_{i=1}^4 \dot{d}_i \quad (65) \end{aligned}$$

Considering the equation (62), the inequation (64) can be rewritten as follows:

$$\dot{V}_e \leq -H_{\min} V_e + 2\tilde{d}_{\max} \quad (66)$$

where $H_{\min} = \min \left[\frac{2(H_{d1} - 1)}{2H_{d4}}, \frac{2H_{d2}}{2(a_1 - 0.5)}, \frac{2(H_{d3} - 1)}{2(a_2 - 0.5)} \right] > 0$ and $\tilde{d}_{\max} = \max [\tilde{d}_{1\max}, \tilde{d}_{2\max}, \tilde{d}_{3\max}, \tilde{d}_{4\max}]$. According to the equation (65), V_e is bounded and $V_e \leq \xi$ in a finite amount of time. Through selecting a large enough H_{\min} , it can ensure that V_e tends to zero. Therefore, the error defined through the equation (61) can converge to any small neighborhood of the original system. As a result, the theorem is proved.

To sum up, the output voltage of the upper/lower arm of the energy interaction converter can be well controlled to $V_u = V_b = V_{ref}^*$, in other word, the output voltage of the energy interaction converter can achieve $V_{out} = V_{ref}$.

IV. CURRENT INNER LOOP PROPORTIONAL-RESONANT CONTROLLER

According to the fixed power and voltage, the output current of the upper arm or below arm regarding the energy interaction converter is fixed ($i_u = i_b = C$). Based on this, the heat loss of the energy interaction converter is $P_{loss} = 0.5 (i_{u1}^2 R + i_{u2}^2 R + i_{u3}^2 R + i_{b1}^2 R + i_{b2}^2 R + i_{b3}^2 R)$. If $i_{u1} = i_{u2} = i_{u3} = 1/3C$ and $i_{b1} = i_{b2} = i_{b3} = 1/3C$, the heat loss of the energy interaction converter is minimum in light of the inequality of arithmetic and geometric means. Therefore, the current sharing modular controller should be proposed to make $i_{u1} = i_{u2} = i_{u3} = 1/3C$ and $i_{b1} = i_{b2} = i_{b3} = 1/3C$. Although the arms of the energy interaction converter are mirror symmetrical, the inevitable deviation of circuit parameters and duty cycle will lead to the inconsistency of current flowing through the six channels, resulting in unnecessary loss and heating of hardware device. Traditionally, PI controller is always used to realize accurate current sharing. Nevertheless, the constant power load is prone to low frequency and sub-synchronous oscillation in electromagnetic timescale. Thus, the current sharing proportional-resonance (PR) controller is adopted in this paper. The detailed control block diagram is shown in Fig. 5 where $i_{ave} = (i_u + i_b) / 6$. Meanwhile, the

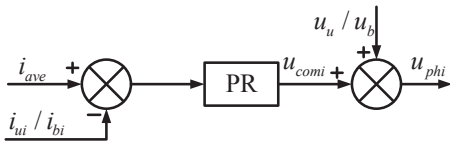


Fig. 5: Current sharing PR controller.

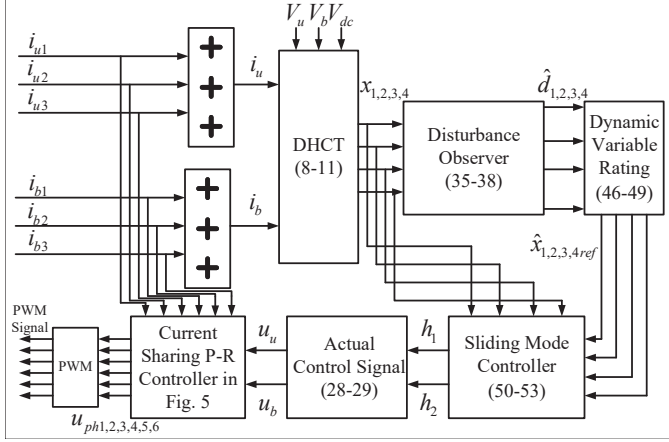


Fig. 6: Overall control block diagram.

current sharing compensator for each path is expressed as follows:

$$u_{comi} = K_P e_{comi} + \frac{K_R s}{s^2 + \omega_c^2} e_{comi} \quad (67)$$

where $e_{comi} = i_{ave} - i_{ui}$ or $e_{comi} = i_{ave} - i_{bi}$; K_P and K_R represent proportional parameter and resonant parameter, respectively. Meanwhile, $K_P > 0$ and $K_R > 0$. Noting that the control bandwidth of sliding mode controller is more than 5 times higher than that of proportional resonant controller [28]. For pure dc current without low-frequency oscillation, PI controller is widely applied, and under this case, $\omega_c = 0$. In the system with weak source and constant power load, low-frequency oscillation whose frequency is below than 5 Hz, should be considered [29]-[30]. In order to improve performance for these low-frequency components (1 to 5 Hz), ω_c is selected as $\omega_c = (1 + 5)/2 = 3Hz$ in this paper. Of course, the plenty of PR controllers ($\omega_i = i$) can be applied to further improve the controller performance.

To sum up, the overall control block diagram of the vehicle-vehicle energy interaction converter is shown in Fig. 6.

V. SIMULATION

The effectiveness of the energy interaction converter controlled through disturbance observer based sliding mode control algorithm is verified by simulation results in this section. In Cases 1-3, the different rated voltage or power vehicles are applied to verify the high application of the proposed method. Furthermore, Case 4 is applied to illustrate the high performance of the proposed method. The selection regarding controller parameter values can be divided into two parts, i.e., PR controller and disturbance observer based sliding model controller. Firstly, in the system with weak source and constant power load, the low-frequency oscillation whose frequency is

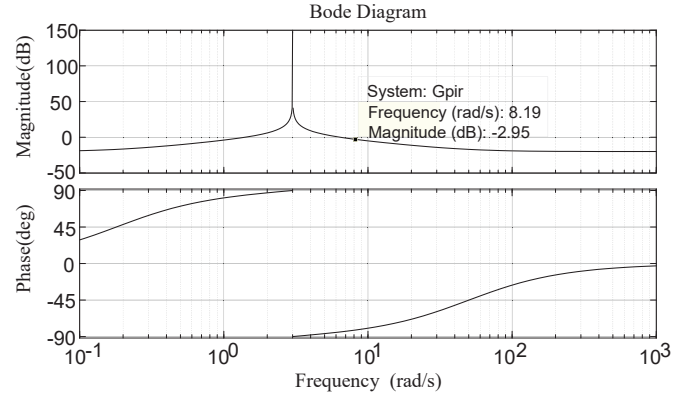


Fig. 7: Bode diagram of the PR controller.

below than 5 Hz, should be considered [29]-[30]. In order to improve performance for these low-frequency components (1 to 5 Hz), ω_c is selected as 3 Hz in this paper. Secondly, the interactive impact between two controllers can be ignored if the control bandwidth of one controller is more than 5 times higher than that of another controller [26]. Therein, the control bandwidth of sliding mode controller is more than 100 Hz. In order to eliminate the interactive impact between two controllers, the control bandwidth of the proposed PR controller should be below than 20 Hz. Based on this, K_P and K_R are selected as $K_P = 0.1$ and $K_R = 5$. As shown in Fig. 7, the control bandwidth of the proposed PR controller is below than 10 Hz. Thirdly, the parameters of disturbance observer based sliding model controller is selected through **Theorem 1**. Under this case, the conditions $((H_{s1} - H_{s2} |s_1|) > (1 + a_1) \sigma_d$ and $(H_{s3} - H_{s4} |s_2|) > (1 + a_2) \sigma_d$ should be satisfied, and one sufficiently large H_{min} should be selected. Firstly, since one sufficiently large H_{min} should be selected, H_{d1} to H_{d4} should be selected as big as possible. Based on this, H_{d1} to H_{d4} can be chosen as $H_{d1} = H_{d3} = 2000$ and $H_{d2} = H_{d4} = 280$. Considering H_{s1} and H_{s3} are positive definite switching gains, which causes the sliding mode controller chattering problem, small H_{s1} and H_{s3} should be chosen. As a result, H_{s1} and H_{s3} can be chosen as $H_{s1} = H_{s3} = 0.01$. Meanwhile, since H_{s2} and H_{s4} can decrease the voltage dip during the load power change, big H_{s2} and H_{s4} should be chosen. As a result, H_{s2} and H_{s4} can be chosen as $H_{s2} = H_{s4} = 20000$. Since a_1 and a_2 can decrease the voltage dip during the load power change, big a_1 and a_2 should be chosen. However, the conditions $((H_{s1} - H_{s2} |s_1|) > (1 + a_1) \sigma_d$ and $(H_{s3} - H_{s4} |s_2|) > (1 + a_2) \sigma_d$ should be satisfied. Hence, a_1 and a_2 can be chosen as $a_1 = a_2 = 10000$. Noting that the red line represents the rated reference value in following simulation test system.

A. Case 1

The practical output voltage of the energy supply vehicle B is 75V, and the ideal voltage of the energy consumption vehicle A is 300V and its capacity is $P_{CPL} = 30kW$. Based on this, the ideal output voltage of the upper/lower bridge arm of the energy interaction converter is $V_{ref}^* =$

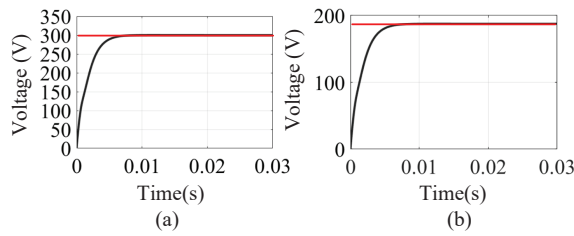


Fig. 8: The voltage of the energy interaction converter under Case 1: (a) actual output voltage; (b) actual output voltage of upper/lower bridge arm.

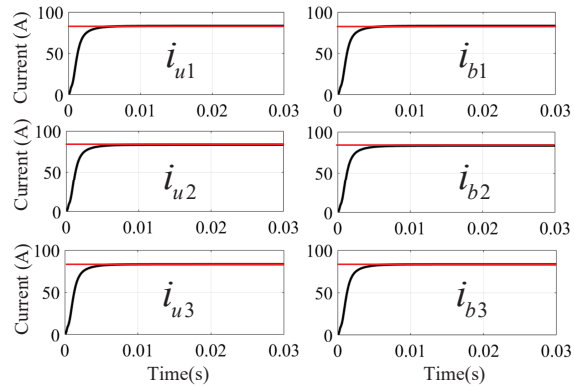


Fig. 9: Each bridge arm current of the energy interaction converter under Case 1.

$(V_{ref} + V_{dc})/2 = 187.5V$, and the ideal output voltage of the energy interaction converter is $V_{ref} = 300V$. From Fig. 8(a), the actual output voltage of the energy interaction converter is $V_{out} = 300V$. From Fig. 8(b), the actual output voltage of the upper/lower bridge arm of the energy interaction converter is $V_u = V_b = (V_{ref} + V_{dc})/2 = 187.5V$. Based on this, the energy interaction converter controlled through disturbance observer based sliding mode control algorithm can provide ideal voltage for the energy consumption vehicle A. Furthermore, the current of each arm regarding energy interaction converter is same, which is shown in Fig. 9. The performance of the current sharing PR controller can be ensured. As a result, the effectiveness of the energy interaction converter controlled through disturbance observer based sliding mode control algorithm has been verified by foresaid simulation results.

B. Case 2

The practical output voltage of the energy supply vehicle B is $60V$, and the ideal voltage of the energy consumption vehicle A is also $300V$ and its capacity is also $P_{CPL} = 30kW$. To this end, the ideal output voltage of the upper/lower bridge arm of the energy interaction converter is $V_{ref}^* = (V_{ref} + V_{dc})/2 = 180V$, and the ideal output voltage of the energy interaction converter is $V_{ref} = 300V$. The actual output voltage of the energy interaction converter is $V_{out} = 300V$, which is shown in Fig. 10(a). As shown in Fig. 10(b), the actual output voltage of the upper/lower bridge arm of the energy interaction converter is $V_u = V_b = (V_{ref} + V_{dc})/2 = 180V$. To this end, the energy interaction converter controlled through

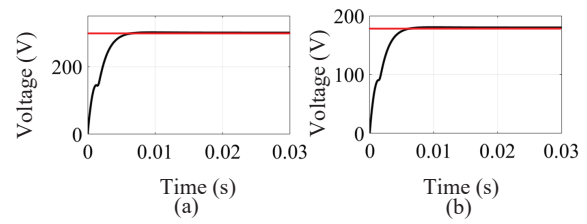


Fig. 10: The voltage of the energy interaction converter under Case 2: (a) actual output voltage; (b) actual output voltage of upper/lower bridge arm.

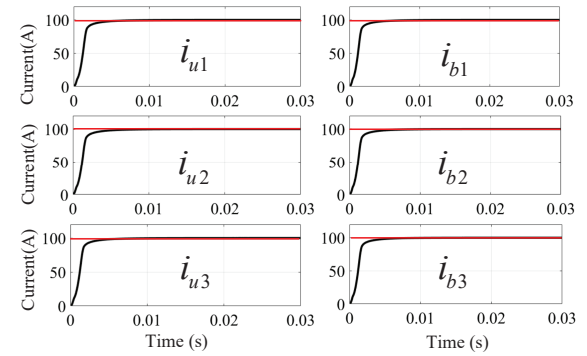


Fig. 11: Each bridge arm current of the energy interaction converter under Case 2.

disturbance observer based sliding mode control algorithm can provide ideal voltage for the energy consumption vehicle A. This conclusion is the same as the conclusion in Case 1. Furthermore, the current of each arm regarding energy interaction converter is also same, which is shown in Fig. 11. The effectiveness of the current sharing PR controller can be also ensured. As a result, the effectiveness of the energy interaction converter controlled through disturbance observer based sliding mode control algorithm has been verified by foresaid simulation results.

C. Case 3

The practical output voltage of the energy supply vehicle B is $60V$, and the ideal voltage of the energy consumption vehicle A is chosen as $250V$ and its capacity is also $P_{CPL} = 20kW$. To that end, the ideal output voltage of the upper/lower bridge arm of the energy interaction converter is $V_{ref}^* = (V_{ref} + V_{dc})/2 = 155V$, and the ideal output voltage of the energy interaction converter is $V_{ref} = 250V$. The actual output voltage of the energy interaction converter is $V_{out} = 250V$, which is shown in Fig. 12(a). As shown in Fig. 12(b), the actual output voltage of the upper/lower bridge arm of the energy interaction converter is $V_u = V_b = (V_{ref} + V_{dc})/2 = 155V$. Thus, the energy interaction converter controlled through disturbance observer based sliding mode control algorithm can provide ideal voltage for the energy consumption vehicle A. This conclusion is the same as the conclusion in Cases 1 and 2. Furthermore, the current of each arm regarding energy interaction converter is also same, which is shown in Fig. 13. The effectiveness of the current sharing PR controller can be ensured. Therefore, the effectiveness of

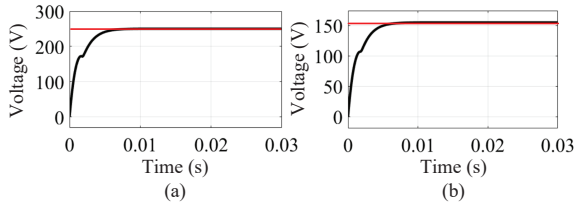


Fig. 12: The voltage of the energy interaction converter under Case 3: (a) actual output voltage; (b) actual output voltage of upper/lower bridge arm.

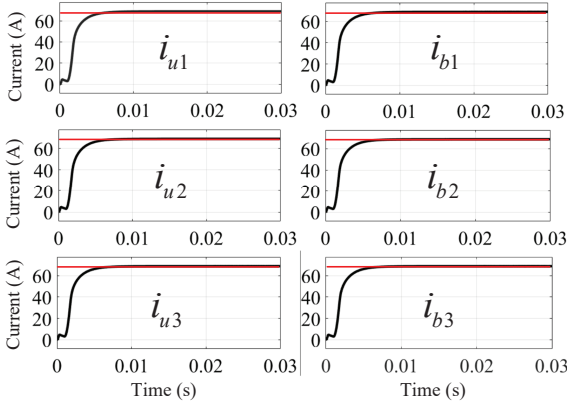


Fig. 13: Each bridge arm current of the energy interaction converter under Case 3.

the energy interaction converter controlled through disturbance observer based sliding mode control algorithm has been verified by foresaid simulation results.

D. Case 4

In order to verify the high performance of the proposed method under different voltage and current of the battery charging, some simulation results are provided, which are shown as follows: Firstly, the ideal voltage of the energy consumption vehicle A is 300V at initial time, and the ideal voltage of the energy consumption vehicle A is 250V at 0.015s. As shown in Fig. 14, the actual output voltage of the energy interaction converter is same as the ideal voltage. Wherein, the main observation values are \hat{d}_1 and \hat{d}_3 . Thus, the time-domain curve of the real values and estimation values regarding \hat{d}_1 and \hat{d}_3 are shown in Figs 15-16. As shown in Figs. 15-16, the observation accuracy can be verified. Furthermore, the ideal voltage of the energy consumption vehicle A is 300V. Therein, the capacity of the energy consumption vehicle A is 20kW at initial time, and the capacity of the energy consumption vehicle A is 30kW at 0.015s. As shown in Fig. 17, the actual output voltage of the energy interaction converter is same as the ideal voltage. Based on this, the high performance of the proposed method under different voltage and current of the battery charging can be verified.

In order to illustrate the performance of the proposed method, one comparison research involves the proposed method and the traditional sliding mode control method, which is shown through (50)-(51). Fig. 18 shows the actual output voltage of the energy interaction converter regulated by the

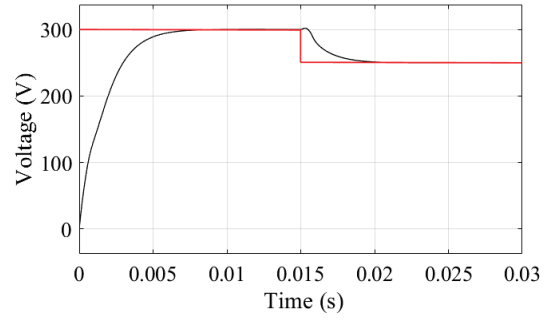


Fig. 14: The actual output voltage of the energy interaction converter under different voltage case.

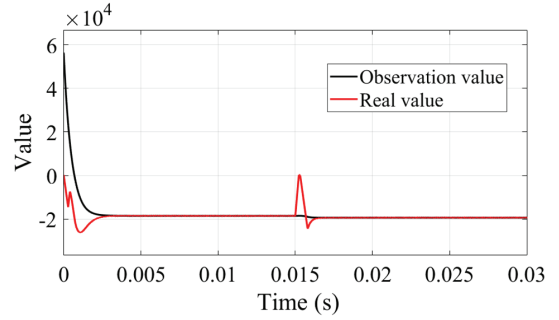


Fig. 15: The relative curves between observation value \hat{d}_1 and real value.

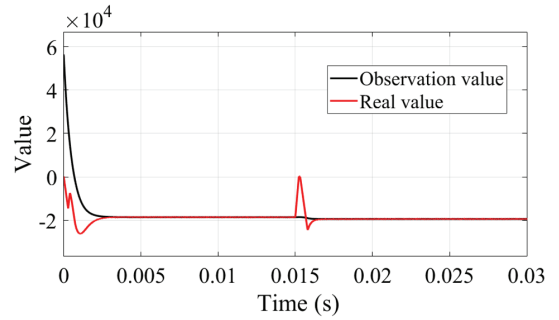


Fig. 16: The relative curves between observation value \hat{d}_3 and real value.

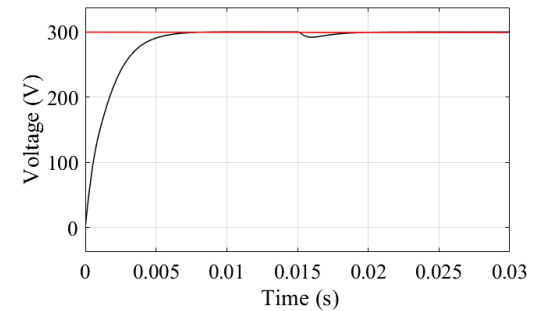


Fig. 17: The actual output voltage of the energy interaction converter under different capacity case.

proposed method (in black) and the traditional sliding mode control method (in blue). Therein, the ideal voltage of the energy consumption vehicle A is 300V. Furthermore, the

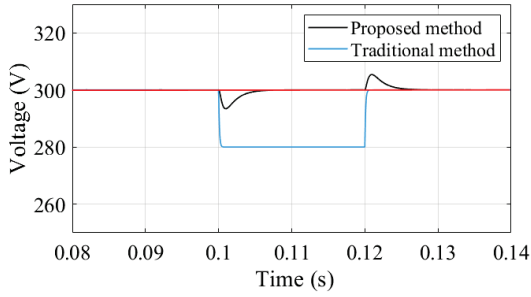


Fig. 18: The actual output voltages of the energy interaction converter obtained through using the proposed method and the traditional method.

capacity of the energy consumption vehicle A is from 30kW to 40kW at 0.1s, and restores to 30kW at 0.12s. Although the values of x_{2ref} and x_{4ref} are selected to satisfy the conditions of $d_1 + x_{2ref} = 0$ and $d_2 + x_{4ref} = 0$ under 30kW, the change regarding 40kW causes an error. As a result, the actual output voltage of the energy interaction converter is 280V from 0.1s to 0.12s, which is controlled through the traditional method. However, the actual output voltage of the energy interaction converter is 300V, which is controlled through the proposed method. Based on this, the high performance of the proposed method can be verified.

VI. EXPERIMENT

In order to verify the high application of the energy interaction converter controlled through disturbance observer based sliding mode control algorithm for vehicles, the controller hardware-in-the-loop (CHIL) experiments are executed in OPAL-RT real-time simulation system with the system parameters, which are the same as the simulation section. The CHIL experiment facility is cited in our previous literature [28]. The detailed experimental figure is shown in Fig. 19. Therein, the control frequency is $10^5 Hz$, and the energy interaction converter is controlled through Digital Signal Processor (DSP) controllers (TMS320F28335). The inputs of DSP are current (i_u and i_b) and voltage (V_u , V_b and V_{dc}) measurements, which are converted from digital signals to the analog signals by the D2A terminals of OPAL-RT system. Furthermore, the outputs of the DSP controllers are pulswidth modulation (PWM) signals, which are sent to the PWM channels of the OPAL-RT system and then drive the power switches in the energy interaction converter model. Finally, the energy interaction converter model is embedded into OPAL-RT OP5600 simulator. Noting that the red line represents the rated reference value in following simulation test system. The practical output voltage of the energy supply vehicle B is 75V, and the ideal voltage of the energy consumption vehicle A is 300V and its capacity is $P_{CPL} = 30kW$. Therefore, the ideal output voltage of the energy interaction converter is $V_{ref} = 300V$. From Fig. 20, the actual output voltage of the energy interaction converter is $V_{out} = 300V$. As a result, the energy interaction converter controlled through disturbance observer based sliding mode control algorithm can provide ideal voltage for the energy consumption vehicle

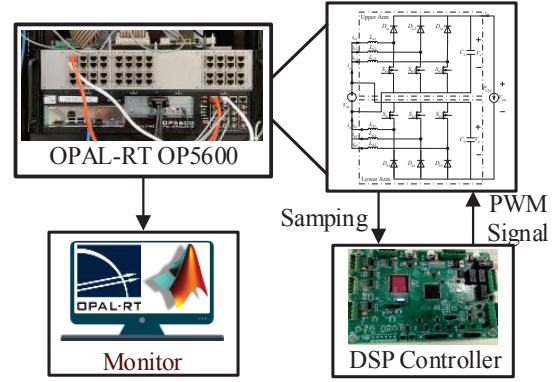


Fig. 19: The CHIL experiment topology.

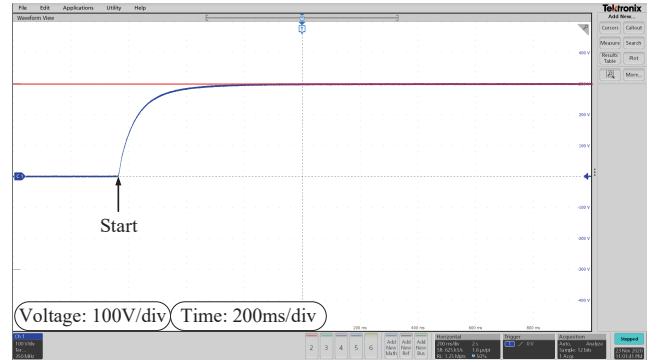


Fig. 20: The actual output voltage of the energy interaction converter under CHIL experiment.

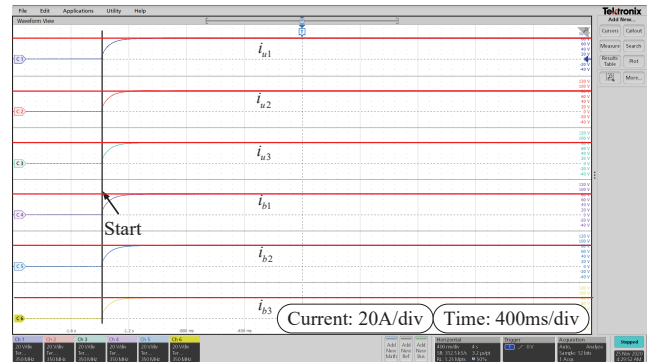


Fig. 21: Each bridge arm current of the energy interaction converter under CHIL experiment.

A. Furthermore, the current of each arm regarding energy interaction converter is same, which is shown in Fig. 21. The performance of the current sharing PR controller can be ensured. As a result, the effectiveness of the energy interaction converter controlled through disturbance observer based sliding mode control algorithm has been verified by the relative experimental results.

VII. CONCLUSION

In order to solve the two main problems which hinder the development of electric vehicles, i.e., charger unavailability and range anxiety, this paper has proposed the energy interaction converter controlled through disturbance observer based

sliding mode control algorithm such that the owner can realize the fast energy mutual assistance between vehicle and vehicle. In view of the low minimum short circuit ratio and high power density, the equivalent six channel interleaved floating dual boost converter and its state-space function have been firstly constructed in this paper. For weak source and constant power load, the disturbance observer based sliding mode control algorithm based on the built state-space function has been proposed to provide constant voltage and power which are in line with the relative standard of electric vehicles. In order to solve the problem of six channel current sharing, the current sharing PR controller has been designed to reduce the heat loss and improve the service life of device. Finally, the simulation and experiment results have been provided to illustrate that the proposed energy interaction converter controlled through disturbance observer based sliding mode control algorithm is effective.

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