

# A New Antenna with Dual Band-Notched Function by Shorting Pin and S-shaped Coupling Element

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**Abstract**—a simple microstrip UWB antenna with dual band-notch function is presented. The antenna consists of a square patch and a partial ground plane. For expanding the impedance bandwidth, H-shaped slot on the ground plane is etched. Also, to obtain two notched bands, S-shaped coupling element and an inverted L-shaped arm ended up a shorting pin are utilized. The antenna has a compact size of  $15 \times 22 \text{ mm}^2$  which has been printed on an FR4 substrate. Moreover, the proposed antenna has been successfully fabricated and measured, indicating broadband matched impedance (2.6-11.4 GHz,  $VSWR \leq 2$ ) and dual band-notched (3.2-4 GHz and 5.1-6.1 GHz) respectively.

**Index Terms**— UWB, Antenna, Notched Band, Shorting pin.

## I. INTRODUCTION

Commercial ultra-wideband (UWB) systems require compact, cheap antennas with omnidirectional patterns and extended bandwidth. It is a popular fact that monopole antennas present really attractive physical features, namely simple structure, small size and low cost. Because of all these interesting characteristics, planar monopoles are quite appealing to be used in emerging UWB applications, and rising research activity is being focused on them. In UWB communication systems, one of main subjects is the design of a compact antenna whilst providing wideband characteristic over the all operating frequency band. Consequently, an enormous number of microstrip antennas with different structures have been experimentally characterized which patch of this type of reported antennas has different shapes such as rectangular, disc, triangle and oval forms [1-5], [17]. There are many techniques on patch, feed line and ground structure to enhance the impedance bandwidth and access to UWB bandwidth [6-7]. The frequency range for UWB systems between 3.1 and 10.6 GHz will end up interference to the existing wireless

communication systems, such as the wireless local area network (WLAN) for IEEE 802.11a operating in 5.15–5.35 GHz and 5.725–5.825 GHz bands, therefore the UWB antenna with a band-stop performance is needful. Newly, to create the frequency band-notch function, modified planar monopoles have been recently presented [8–12]. According to it, the antenna presented in [8] has been designed by embedding a pair of T-shaped stubs in the radiation patch and a modified G-slot defected ground structure in the feeding line, [9-10] use traditional method of U-shaped slot on the patch, and [11] applies T-shaped stub embedded in the square slot of the radiation patch and a pair of U-shaped parasitic strips beside the feed line. At the end of paper using Table 2, the antenna is compared to references [8-11], [17].

## II. ANTENNA DESIGN AND RESULTS

The configuration and photo of the fabricated antenna are shown in figure 1, which has been printed on an FR4 substrate with thickness 1mm and permittivity 4.4. To connect a 50- $\Omega$  SMA connector for signal transmission, the width of the microstrip feedline,  $W_f$ , is fixed at 1.9 mm. The basic antenna structure contains a square patch, a feedline, and a partial ground plane. On the other side of the substrate, a conducting ground plane with width  $W_{sub}$  and length  $L_{gnd}$  is situated. The ground plane with an H-shape plays an important role in the broadband characteristics of this antenna, because it can adjust the electromagnetic coupling effects between the patch and the ground plane, and improve its impedance bandwidth without any cost of size or expense. To achieve two notched bands, two diverse techniques have been used, the former S-shaped coupling element on the back side and the latter an inverted L-shaped arm ended up a shorting pin.

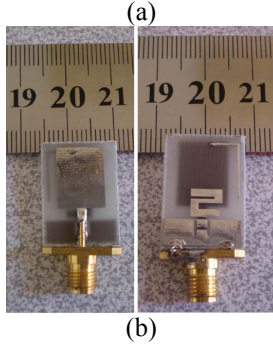
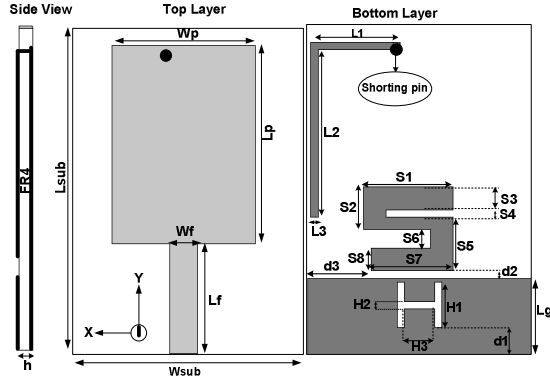


Fig. 1. Geometry (a) and photo (b) of the fabricated antenna

Table 1. Optimal Dimensions of the Antenna

Prm.	(mm)	Prm.	(mm)	Prm.	(mm)	Prm.	(mm)
$L_{sub}$	22	$W_{sub}$	15	$W_p$	10	$L_p$	13.5
$W_f$	1.9	$L_f$	7.5	$L_g$	5	$L_1$	6
$L_2$	11	$L_3$	0.5	$S_1$	6	$S_2$	2.8
$S_3$	1.5	$S_4$	0.5	$S_5$	3.5	$S_6$	1.2
$S_7$	5.5	$S_8$	1.5	$H_1$	3	$H_2$	0.5
$H_3$	2	$d_1$	1.75	$d_2$	0.5	$d_3$	4.25

### III. ANTENNA PERFORMANCE AND DISCUSSION

Computation of the dispersion when the antenna radiates a pulse signal is also of interest. The transmit transfer functions of the antennas were used to compute the radiated pulse in different directions when a reference signal was applied at the antenna input. This signal should present an UWB spectrum covering the antenna bandwidth and particularly the FCC mask from 3.1 to 10.6 GHz. It is shown in figure 2 that an acceptable approximation to a FCC mask compliant pulse can be obtained with a Gaussian seventh derivative. This pulse is represented in the time domain by:

$$G(t) = A \cdot \exp\left(\frac{-t^2}{2\delta^2}\right) \quad (1)$$

$$\begin{aligned} G^n(t) &= \frac{d^n G}{dt^n} \\ &= (-1)^n \frac{1}{(\sqrt{2}\delta)^2} \cdot H_n\left(\frac{t}{\sqrt{2}\delta}\right) \cdot G(t) \end{aligned} \quad (2)$$

$$H_7(t) = 128t^7 - 1344t^5 + 3360t^3 - 1680t \quad (3)$$

This signal and its spectrum are represented in figure 2. The pulse bandwidth is exactly into mask desired.

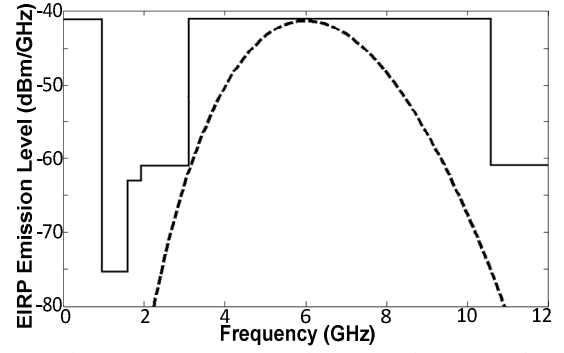


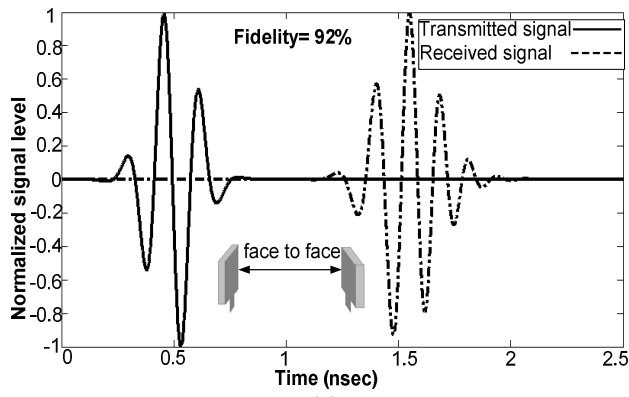
Fig. 2. Power Spectrum Density compared to FCC mask

Luckily, after drawing various Gaussian pulses from the first to eighth derivative, it was obtained that the best pulse for covering FCC mask can be the seventh derivative. Besides, with a bit tolerance, the sixth and eighth derivative are acceptable. In telecommunications systems, the correlation between the transmitted (TX) and received (RX) signals is evaluated using the fidelity factor (4):

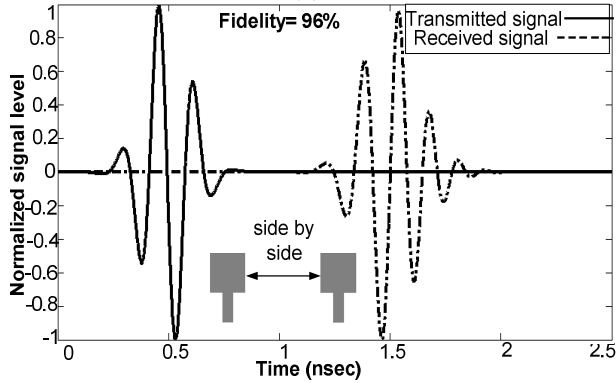
$$F = \max_{\tau} \left| \frac{\int_{-\infty}^{+\infty} S(t)r(t-\tau)dt}{\sqrt{\int_{-\infty}^{+\infty} S(t)^2 \cdot \int_{-\infty}^{+\infty} r(t)^2 dt}} \right| \quad (4)$$

Where  $S(t)$  and  $r(t)$  are the TX and RX signals, respectively.

For impulse radio in UWB communications, it is necessary to have a high degree of correlation between the TX and RX signals to avoid losing the modulated information. However, for most other telecommunication systems, the fidelity parameter is not that relevant. In order to evaluate the pulse transmission characteristics of the antenna in the case of without notch, two configurations (side-by-side and face-to-face orientations) were chosen. The transmitting and receiving antennas were placed in a distance  $d=25\text{cm}$  from each other [14]. As shown in figures 3, although the received pulses in each of two orientations are broadened, a relatively good similarity exists between the RX and TX pulses. Using (4), the fidelity factor for the face-to-face and side-by-side configurations was obtained equal to 0.92 and 0.96, respectively. These values for the fidelity factor show that the antenna imposes negligible effects on the transmitted pulses. The pulse transmission results are obtained using CST [15]. Phase of  $S_{21}$  for the face to face and side by side orientations are also illustrated in figure 4. As previously expected, the plot shows a linear variation of phase in the total operating band except notched bands.



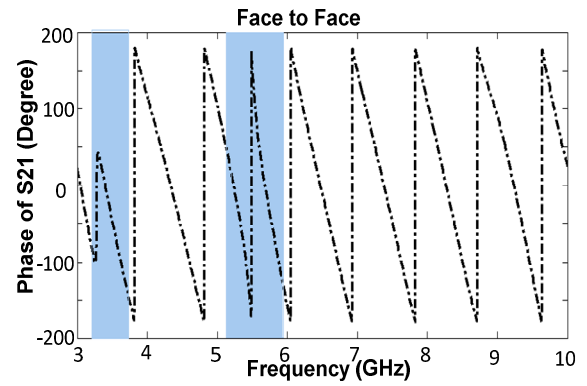
(a)



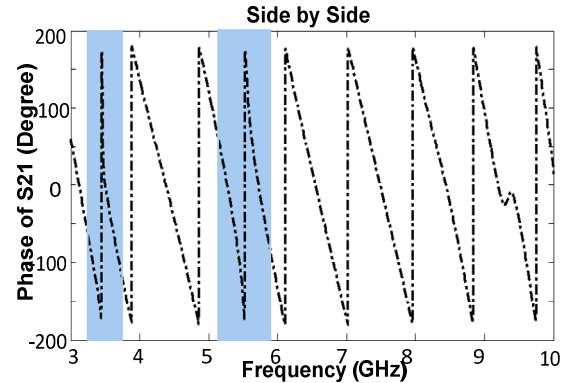
(b)

Fig. 3. Transmitted and received pulses in time domain for a UWB link with identical antennas without notches in (a) face to face and (b) side by side orientations

The parameters of the antenna are studied by changing one parameter at a time and fixing the others. The simulated results are achieved using the Ansoft simulation software high-frequency structure simulator [16]. The optimal dimensions of the designed antenna are demonstrated in Table 1. Figures 5 and 6 exhibit simulated VSWR for the various structures of monopole antenna. With the use of H-shaped slot the bandwidth can be increased markedly, creating the third resonance at 10 GHz, expanding the bandwidth by 10.8 GHz. Meanwhile, S-shaped coupling element on the back side not only can generate a notched band at center frequency 5.5 GHz, but also can rise the bandwidth on the upper band approximately 0.8 GHz. From figure 6 is seen that an inverted L-shaped arm ended up a shorting pin have effect on notched band at center frequency 3.5 GHz while the S-shaped coupling element can produce a stop band at center frequency 5.5 GHz to filter WLAN and WiMAX bands respectively. Besides, it is found out that both notches are independent than each other, it means that they have no effect on each other. As depicted in figure 7, parameter S7 has a noticeable influence on frequency shifting. According to it, with increasing length of S7 the center frequency is decreased regularly in a way that with rising 0.5 mm in length S7 the centre frequency of notched band is reduced approximately 0.5 GHz. The best value S7 for covering 5.15 to 5.825 corresponds to 5.5 mm.



(a)



(b)

Fig. 4. Simulated phase S21 with a pair of identical antennas for (a) face to face (b) side by side orientations.

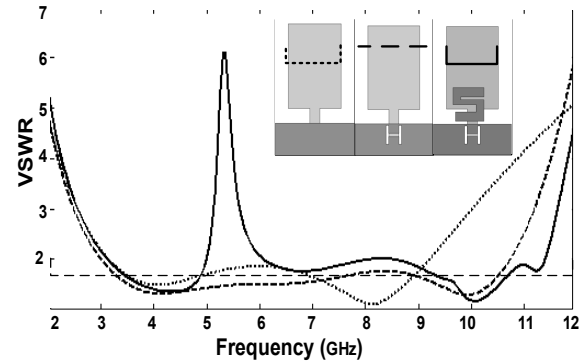


Fig. 5. Simulated VSWR for the various structures of monopole antenna showing wide impedance bandwidth

As said above, in this study to generate the band-stop performance on WiMAX band with center frequency 3.5 GHz, an inverted L-shaped arm, with length of  $L1+L2$ , connected to a shorting pin is used. The simulated VSWR curves with different values  $L2$  are plotted in figure 8. When the length  $L2$  increases gradually the center frequency of the notched band is diminished steadily. Thus, the optimized  $L2$  is 11 mm. From these results, it can be concluded that the notch frequencies are controllable by changing the lengths  $S7$  and  $L2$ . To understand more clearly, figure 9 is used showing the simulated current distributions on both the sides of the antenna.

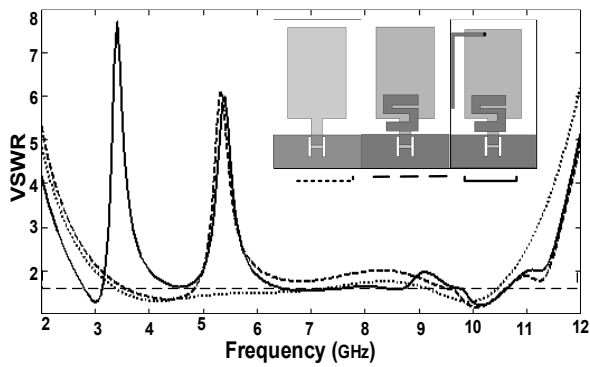


Fig. 6. Simulated VSWR for the various structures of monopole antenna showing notched bands

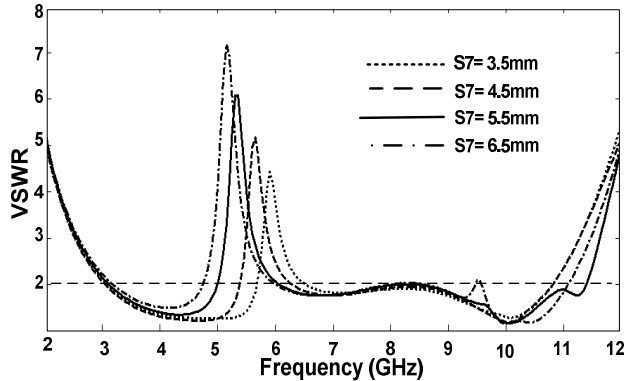


Fig. 7. Simulated VSWR characteristics of the antenna with the S-shaped coupling element with different values S7

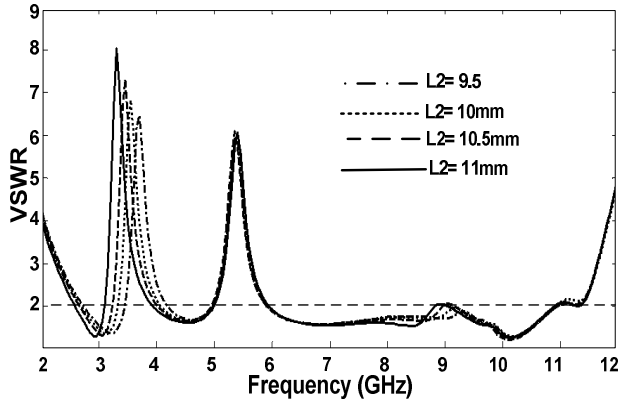


Fig. 8. Simulated VSWR characteristics of the antenna with an inverted L-shaped arm ended up shorting pin with different values L2

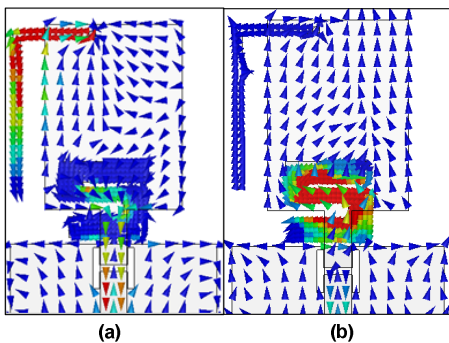


Fig. 9. Simulated surface current distributions (a) on the L-shaped arm ended up shorting pin at 3.5GHz and (b) on S-shaped coupling element at 5.5 GHz

It can be observed in figure 9(a), by using an inverted L-shaped arm ended up shorting pin, the current is concentrated on the arm at 3.5 GHz. Further point that, the current direction on the edge of patch is opposite, 180 degree phase difference, to its direction on L-shaped arm. Figure 9(b) depicts the current distribution at 5.5GHz in a way that most of the current is seen on S-shaped coupling element indicating its effect in creating the second notched band at centre frequency 5.5GHz. Figure 10 shows the measured and simulated VSWR characteristics of the proposed antenna. The fabricated antenna can cover the frequency band of 2.6 to over 11.4 GHz. The designed antenna has a small size of  $15 \times 22 \text{ mm}^2$  while showing the band rejection performance in the frequency bands of 3.2 up to 4 GHz and 5.1 to 6.1 GHz respectively. As displayed in figure 10, there is a discrepancy between measured result and the simulated data, it is more likely because of the effect of the SMA port. Figure 11 illustrates the simulated radiation patterns constituting the co-polarization and cross-polarization in the H-plane ( $x-z$  plane) and E-plane ( $y-z$  plane). It can be seen that the radiation patterns in  $x-z$  plane are about omnidirectional for the two frequencies while radiation pattern in  $y-z$  plane are nearly directional.

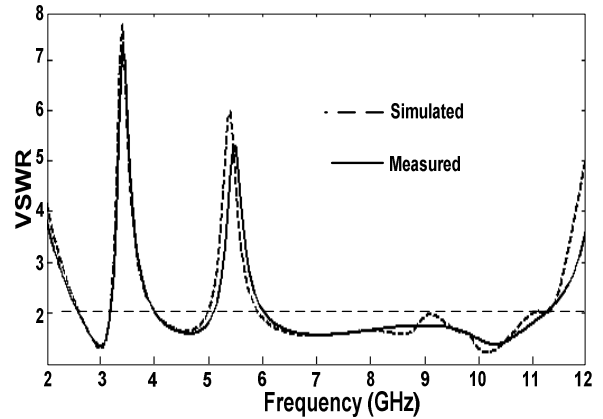


Fig. 10. Measured and simulated VSWR characteristics for the proposed antenna

The comparisons for several different dual-notched-band UWB antennas are illustrated in Table 2. Compared to [8-11], the proposed UWB antenna with dual notched bands in terms of size and bandwidth has better characteristics. Further point, the used techniques for increasing impedance bandwidth and obtaining notched bands in the proposed antenna are newer than methods mentioned in the references.

Table 2. Comparisons of the UWB Antenna to other UWB Antennas

Performance compare	The Ant.	Ref [8]	Ref[9]	Ref [10]	Ref [11]
Dielectric constant	4.4	4.4	2.65	4.4	3.38
Thickness (mm)	1	1	1	1.6	0.8
Size (mm)	22×15	41×34	15×22	30×26	32×26
Bandwidth (GHz)	2.6-11.4	2.8-11.8	2.9-12	3-11	2.8-11

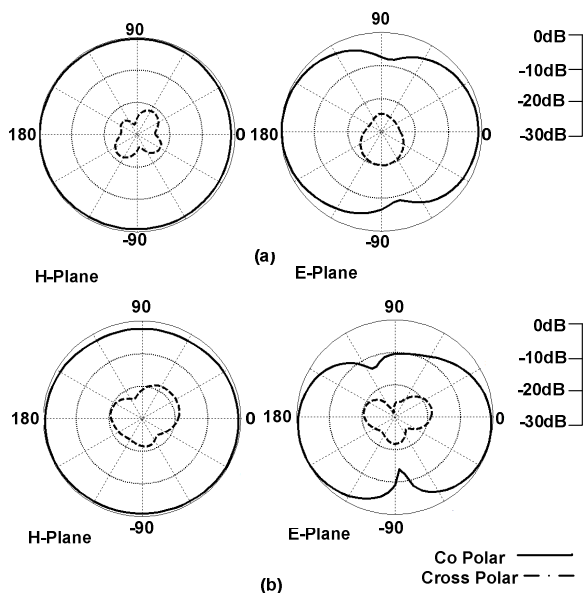


Fig. 11. Radiation patterns of the antenna at (a) 4.5 and (b) 8 GHz

#### IV. CONCLUSION

In this paper, a new microstrip antenna with extended bandwidth capability for UWB applications was presented. In this design, the antenna can operate from 2.6 to 11.4 GHz with  $VSWR \leq 2$  and displays a good omnidirectional radiation pattern even at higher frequencies. The designed antenna has a small size of  $15 \times 22 \text{ mm}^2$  while showing the band rejection performance in the frequency bands of 3.2 to 4 and 5.1 to 6.1 GHz, respectively. The paper mentions to a valuable point including the use of the seventh derivative of Gaussian pulse for covering FCC mask. Good VSWR and radiation pattern characteristics are obtained in the frequency band of interest.

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