

Experimental Demonstration of Dual-polarisation NFDm Transmission with b -Modulation

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Abstract—Dual-polarisation Nonlinear Frequency Division Multiplexing (DP-NFDM) transmission has been intensively investigated recently due to its potential of doubling the capacity in comparison to single polarisation NFDM systems. However, up to now, due to many challenges in design and practical implementation, demonstrated data rates of DP-NFDM transmission systems in experiments are still much lower than the record data rate of single polarisation NFDM transmissions (125 Gb/s). In this work, by employing the concept of b -modulation and developing effective digital signal processing (DSP), we have experimentally demonstrated for the first time a high capacity DP-NFDM transmission system, achieving a net data rate of 220 Gbps with spectral efficiency (SE) of 4 bits/s/Hz.

Index Terms—Non-linear Fourier transform, non-linear frequency-division multiplexing, non-linear transmission scheme.

I. INTRODUCTION

NFDM has been proposed as a potential technique to combat the fibre Kerr non-linearity impairment, which imposes a limitation on the achievable throughput (or SE) of conventional fibre communication systems [1]. The key idea of NFDM transmission is to encode information onto the nonlinear signal spectrum (defined by the Nonlinear Fourier Transform (NFT)) which evolves linearly along the loss-less fibre channel [2]. In this case, the deterministic nonlinear cross-talks among nonlinear spectral components are absent, which potentially leads to higher SE. For the simplicity, the concept of NFDM has been firstly considered for single polarisation transmissions [3]. Many techniques for encoding and transmitting information using the nonlinear spectrum have been investigated [4]–[9]. In addition, many research groups have put a lot of efforts in demonstrating NFDM transmission systems experimentally [10]–[12]. Many encouraging results have been reported, showing that data rates beyond 100 Gbps per channel can be achieved. The highest data rate so far of a single polarisation NFDM transmission is 150 Gbps gross data rate over 976 km [4], which was achieved by modulating simultaneously 222 nonlinear spectral components

(or nonlinear modes). Further increasing the data rate requires increasing the number of modulated nonlinear modes, which has been shown to be challenging due to the nonlinear cross-talks among nonlinear modes in the presence of ASE noise, fibre loss and implementation imperfections [13]. Another effective way to increase the data rate of NFDM transmission is to extend the concept of NFDM to dual polarisation transmission. In recent year, some proof of concept DP-NFDM transmission systems, both in simulation [9] and experiments [10] have been reported. However, high capacity DP-NFDM transmission have not been reported yet. In our previous work [14], we simulated the b -modulated DP-NFDM transmission system, and carefully optimised it for high data rate. We showed that the SE of b -modulated system achieved 1.2 bits/s/Hz higher SE than q_c -modulated system. In this work, we experimentally implemented a DP-NFDM transmission system simulated in [14]. By developing efficient DSP, we could successfully modulate 196 nonlinear sub-carriers in each polarisation, achieving a net data rate of 220 Gbps over 976 km of EDFA-based fibre link. To the best of our knowledge, this is the highest data rate of any NFDM systems in experiment up to date as shown in Fig. 1.

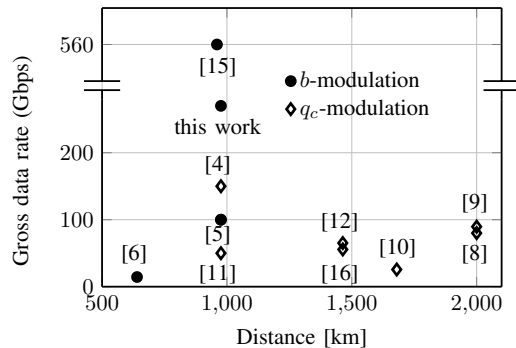


Fig. 1. Gross data rate of recently implemented NFDM systems with q_c - or b -modulation.

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II. THE DP-NFDM SIGNAL GENERATION

In this section, we outline the NFT framework and discuss the DP-NFDM signal generation in brief. In NFDM system, the information is encoded on the non-linear spectra that consist of the continuous spectrum ($q_{ci}(\lambda)$, $\lambda \in \mathbb{R}$, $i = 1, 2$) and the discrete spectrum (eigenvalues $\lambda_m \in \mathbb{C}^+$ and their spectral amplitude $q_{di}(\lambda_m)$, $m = 1, 2, 3, \dots, M$). It is also equivalent to

TABLE I
RECENT RESULTS OF NFDm SYSTEMS.

		Cont.		Disc.		Both
		q_c	b	q_d	b_k	
Sim.	SP	[8]		[19]		[20]
	DP	[9]	[15]	[21]	[22]	
Exp.	SP	[4], [7], [11]	[5]	[23], [24]		[16]
	DP	[10]	[6]		[25]	[26]

encode information on the $\{\lambda_m, b_i(\lambda), b_{mi}(\lambda_m)\}$, as they are in one-to-one correspondence to $\{\lambda_m, q_{ci}(\lambda), q_{di}(\lambda_m)\}$ [17, p. 57, Eq. (1.6.19)]. Furthermore, modulating b -coefficient allows us to control the time duration of the INFT signal [18]. We categorise some recent implementations of NFDm systems in Tab. I in terms of the type of modulation, single- or dual-polarisation (SP or DP), and simulation or experiment.

The most important property of the non-linear spectra is that over the noiseless and loss-less non-linear Manakov equation, its evolution can be described by simple equations:

$$\begin{cases} \lambda_m(L) = \lambda_m(0), \\ b_{mi}(L, \lambda_m) = b_{mi}(0, \lambda_m) e^{4j\lambda_m^2 L}, & \lambda_m \in \mathbb{C}^+, \\ b_i(L, \lambda) = b_i(0, \lambda) e^{4j\lambda^2 L}, & \lambda \in \mathbb{R}, \end{cases}$$

where L is the total distance, i the polarisation index, and $\{\lambda_m(0), b_{mi}(0, \lambda_m), b_i(0, \lambda)\}$ the non-linear spectra of the transmitted signal. One can see from the above equations that the spectral amplitude on different non-linear frequency evolves independently during signal propagation in the fibre channel. Therefore, it was proposed in [3] to use an OFDM-like continuous spectrum for NFDm signal generation, as it is written below

$$u_i(\lambda) = \sum_{k=-N_C/2}^{k=N_C/2} c_{ki} \frac{\sin(\lambda T_0 + k\pi)}{\lambda T_0 + k\pi}, \quad i = 1, 2,$$

where T_0 is the NFDm symbol duration, N_C is the number of sub-carriers, and c_{ki} is the data on k th sub-carrier on i th polarisation. The discrete spectrum is not used here.

Since the continuous spectrum generates dispersive waves that broaden in the fibre channel, a guard interval (GI) between NFDm symbols in time domain is necessary to avoid inter-symbol interference (ISI). The GI insertion is done by zero-padding in the inverse Fourier domain of $\{u_1(\lambda), u_2(\lambda)\}$.

To overcome the limiting constraint $|b_1(\lambda)|^2 + |b_2(\lambda)|^2 < 1$ for b -modulation, we apply the following transform Γ_b on the $\{u_1(\lambda), u_2(\lambda)\}$

$$\begin{aligned} \Delta &= \sqrt{1 - e^{(-|u_1(\lambda)|^2 - |u_2(\lambda)|^2)} / (|u_1(\lambda)|^2 + |u_2(\lambda)|^2)} \\ b_1 &= \Delta \cdot u_1(\lambda), \quad b_2 = \Delta \cdot u_2(\lambda). \end{aligned}$$

A detailed discussion about the positive and negative effects of the transform Γ_b can be found in [14]. The resulted non-linear spectrum $\{b_1(\lambda), b_2(\lambda)\}$ will be used to calculate $a(\lambda)$ and subsequently $\{q_{c1}(\lambda), q_{c2}(\lambda)\}$ via

$$\begin{aligned} a(\lambda) &= \sqrt{1 - |b_1(\lambda)|^2 - |b_2(\lambda)|^2} e^{j\mathcal{H}(\frac{1}{2} \log(1 - |b_1(\lambda)|^2 - |b_2(\lambda)|^2))} \\ q_{ci}(\lambda) &= b_i(\lambda) e^{-2j\lambda^2 L / a(\lambda)}, \quad i = 1, 2. \end{aligned} \quad (1)$$

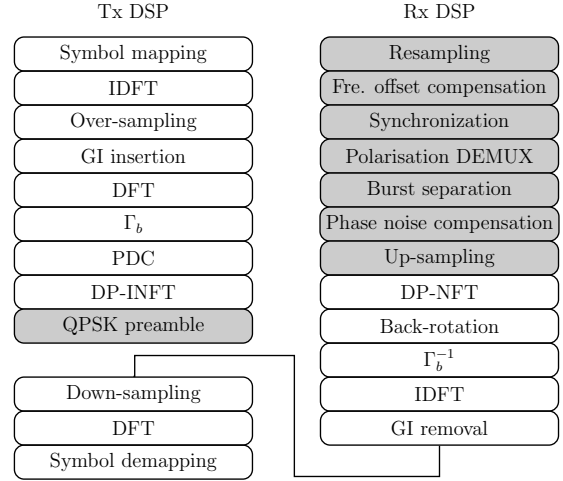


Fig. 2. Transceiver DSP chain.

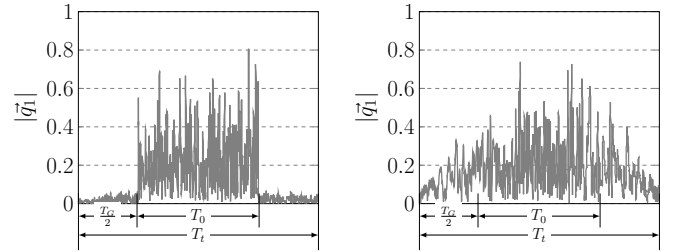


Fig. 3. A realisation of INFT symbols (left) without PDC (right) with PDC.

To reduce the necessary GI to its half, the Pre-Dispersion Compensation (PDC) [27] ($e^{-2j\lambda^2 L}$ phase-rotation of the non-linear spectra) is commonly used at the last step of the spectrum generation as in (1). $\{q_{c1}(\lambda), q_{c2}(\lambda)\}$ will be passed to DP-INFT [9, Sec. 3] to generate the time domain signal. We summarise the detailed signal generation and detection steps in white blocks in Fig. 2.

In this work, we transmit DP-NFDm signals of roughly 55 GHz (N_C/T_0) linear bandwidth. c_{ki} is randomly drawn from a 32-QAM constellation. The guard interval T_G between DP-NFDm symbols is estimated by $T_G \approx \pi W \beta_2 L_{sp} N_{sp} = 3.57$ ns. We set the burst duration $T_0 = T_G$ for simplicity (instead of $T_0 = 5T_G$ for maximum data rate as in [14]). It results in $N_c = 196$ sub-carriers in the non-linear frequency domain. The system loses half of the SE due to the guard interval. The loss can be reduced by increasing T_0 . We show one of the signal realisations in Fig. 3.

III. EXPERIMENTAL SETUP AND DSP

For the transmission experiment, at transmitter, we use four digital-analog converters (DAC) and a polarisation-division multiplexing I/Q modulator to generate the waveform. The output signal is subsequently amplified by an EDFA. Signals are then coupled in and out of the recirculating loop by a 50:50 coupler and travel three loops in our experiment. Each loop has three spans of SMF-28 (Corning) and three EDFAs, making the total distance of the experiment 975.6 km. We chose the same distance as in [4] to allow a direct comparison.

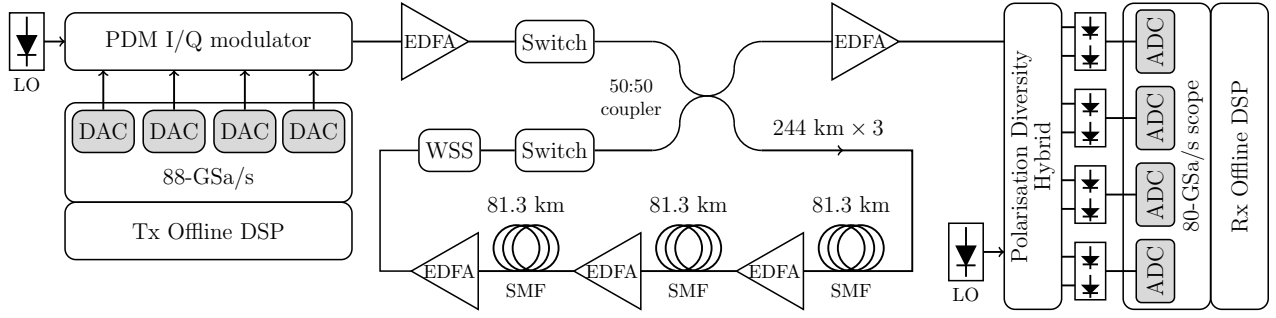


Fig. 4. Recirculating fibre loop experiment setup. The fibre is Corning SMF-28.

As receiver, preceded by another EDFA, an oscilloscope (DSOZ334A) with four channels is used. The sampled data taken by the oscilloscope are saved and processed offline. Two external cavity lasers are used as the optical carrier at the transmitter and as the local oscillator at the receiver. The WSS functions as a optical band-pass filter to remove the out-of-band amplified spontaneous emission noise. Some important parameters of the devices are listed in Tab. II.

TABLE II
SYSTEM PARAMETERS

fibre type	Corning SMF-28
DSP oversampling rate (Tx/Rx)	8
EDFA noise figure	5.5 dB
cavity laser linewidth	100 kHz
DAC Effective number of bits	4.5 ~ 5

Several DSP blocks, marked in gray colour in Fig. 2, are added to deal with synchronisation, frequency-offset compensation, arbitrary polarisation rotation and tracking, and phase noise of the laser. In the following, we explain every ‘gray’ step in the DSP in detail.

1) *QPSK preamble*: For synchronisation and polarisation-demultiplexing (POL-DEMUX) purposes, single-carrier QPSK signals (55 Gbaud Root-raised cosine pulses with roll-off factor of 0.5) are prepended to the DP-NFDM signals. The QPSK signals occupy 4.3% of the transmission period. The choice is motivated by the existence of versatile adaptive filters for POL-DEMUX and detection of QPSK signals. The resulted signal in one duty cycle is illustrated in Fig. 5. The NFDM training sequence is to remove any scaling or phase rotation in the non-linear frequency domain.

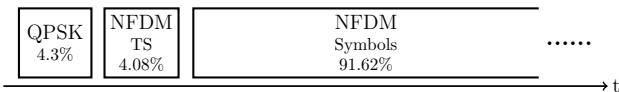


Fig. 5. Signal structure in one duty cycle. TS stands for training symbols.

2) *Frequency Offset Compensation*: The frequency offset compensation was done with the help of the residual carrier.

3) *Synchronisation*: The QPSK preambles are used for synchronisation. The chromatic dispersion (CD) compensation is first applied to the whole signal. By calculating the cross-correlation between the amplitude of the known QPSK ‘pilot’ and the amplitude of the CD-compensated signal, the beginning of the DP-NFDM signal can be easily located.

4) *POL-DEMUX*: The recursive least square multi-sample per symbol constant-modulus algorithm (RLS-msps-CMA) [28, Sec. V-3]) was performed on the CD-compensated QPSK ‘pilot’ to estimate the 2×2 MIMO filter that tracks the arbitrary polarisation rotation and compensates the residual ISI. The obtained filter is then applied on the non-compensated DP-NFDM signals. Without phase noise compensation, a ring constellation is expected from the RLS-CMA.

5) *Phase Noise Compensation*: The phase noise is assumed to be perfectly tracked, and constant within one DP-NFDM symbol. The assumption is realised by comparing the phase of the theoretical waveform (from the noiseless simulation) with the received one, then average within one symbol period. It is equivalent to compensate in the non-linear frequency domain as $e^{j\phi} q(t) \leftrightarrow e^{-j\phi} \{q_{c1}(\lambda), q_{c2}(\lambda)\}$.

IV. EXPERIMENTAL RESULTS

To verify our transceiver DSP chain, we first carried out a back-to-back experiment. The waveforms generated by INFT for each launch power are different. In our back-to-back experiment, however, the transmitted signal power is fixed (set by the EDFA following I/Q modulator). We change only the waveform that is designed for its particular launch power. To collect statistics, we collect at every designed launch power 5 traces of 512 NFDM symbols, each having 196 sub-carriers. The Signal-to-Noise Ratios (SNRs) of the received signal can be calculated from the error vector magnitude (EVM). Fig. 6(a) shows the measured SNR and their average in terms of the designed launch power at the receiver in the back-to-back scenario. It can be seen that, when we use the waveforms designed for launch power larger than -3 dBm, the measured SNR starts to decrease. This is attributed to the reduced accuracy of INFT-NFT algorithm at high power, and DAC quantisation noise.

We perform the transmission experiment over 12 spans of 81.3 km SMF. Waveforms are launched at their designed launch powers, and the polarisation state is also randomly changed at the transmitter. Fig. 6(b) shows the measured SNRs and their average in terms of the launch power. To compute the SE, we estimate the Mutual Information (MI) (of individual sub-carrier detection) by assuming the channel conditional distribution as a Gaussian distribution [29]. The net data rate and SE are computed by

$$\text{Net rate} = \frac{\text{MI} \cdot N_c \cdot 2}{(T_0 + T_G) \text{ ns}} \text{ (Gb/s)}, \quad \text{SE} = \frac{\text{Net rate}}{55 \text{ GHz}} \text{ (bits/s/Hz)}.$$

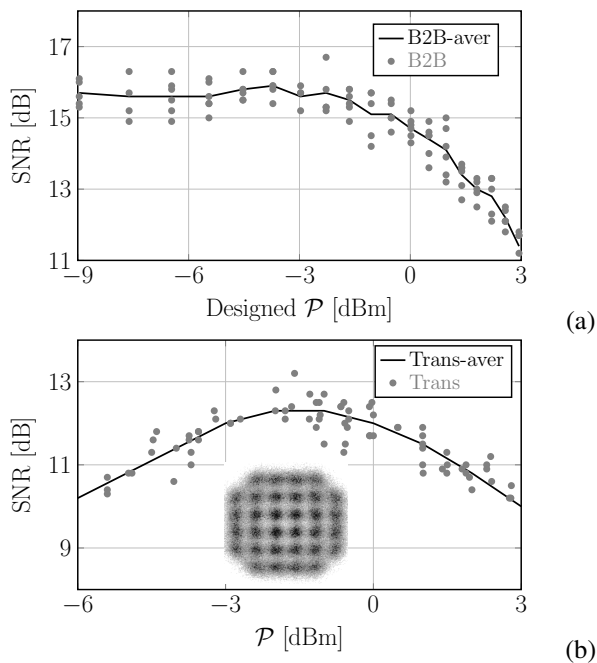


Fig. 6. Measured SNRs and their average (a) in terms of the designed launch power in the back-to-back scenario, (b) in terms of the launch power over 12 spans of 81.3 km SMF. Below the curve is one received constellation at signal power of -1.3 dBm, Q factor = 3.7 dB, SE \approx 2 bits/s/Hz/pol.

This net data rate can be achieved by a soft-decision capacity-approaching binary code such as spatially coupled LDPC codes [30]. At the launch power of -1.3 dBm, the system reached its maximum net rate—220 Gbps, SE of 4 bits/s/Hz. The corresponding constellation is also plotted in Fig. 6(b).

V. CONCLUSIONS

In summary, we demonstrate in experiment a 220 Gbps b-modulated DP-NFDM system, achieving a SE of 4 bits/s/Hz. We experimentally verified the system design developed in [15], and added extra DSP blocks to handle frequency offset compensation, synchronisation, POL-DEMUX and phase noise compensation through a QPSK ‘pilot’ preamble. The data rate can potentially be improved by increasing the number of sub-carrier in each DP-NFDM symbol.

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